

FEATURES

- 18-bit resolution with no missing codes**
- Throughput: 1 MSPS**
- Low power dissipation**
 - 4 mW at 1 MSPS (VDD only)
 - 7 mW at 1 MSPS (total)
 - 70 μ W at 10 kSPS
- INL: ± 1 LSB typical, ± 2 LSB maximum**
- Dynamic range: 99 dB**
- True differential analog input range: $\pm V_{REF}$**
 - 0 V to V_{REF} with V_{REF} between 2.5 V to 5.0 V
 - Allows use of any input range
 - Easy to drive with the ADA4941
- No pipeline delay**
- Single-supply 2.5 V operation with 1.8 V/2.5 V/3 V/5 V logic interface**
- Serial interface SPI[®]-/QSPI[™]-/MICROWIRE[™]-/DSP-compatible**
- Ability to daisy-chain multiple ADCs and busy indicator**
- 10-lead package: MSOP (MSOP-8 size) and 3 mm \times 3 mm QFN (LFCSP), SOT-23 size**

APPLICATIONS

- Battery-powered equipment**
- Data acquisition systems**
- Medical instruments**
- Seismic data acquisition systems**

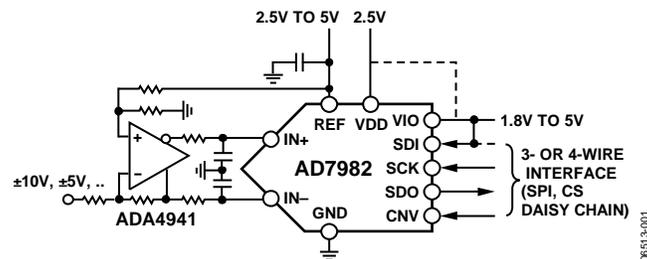
APPLICATION DIAGRAM EXAMPLE


Figure 1.

GENERAL DESCRIPTION

The AD7982 is an 18-bit, successive approximation, analog-to-digital converter (ADC) that operates from a single power supply, VDD. It contains a low power, high speed, 18-bit sampling ADC and a versatile serial interface port. On the CNV rising edge, the AD7982 samples the voltage difference between the IN+ and IN- pins. The voltages on these pins usually swing in opposite phases between 0 V and V_{REF} . The reference voltage, REF, is applied externally and can be set independent of the supply voltage, VDD. Its power scales linearly with throughput.

The SPI-compatible serial interface also features the ability, using the SDI input, to daisy-chain several ADCs on a single 3-wire bus and provides an optional busy indicator. It is compatible with 1.8 V, 2.5 V, 3 V, and 5 V logic, using the separate VIO supply.

The AD7982 is available in a 10-lead MSOP or a 10-lead QFN (LFCSP) with operation specified from -40°C to $+85^{\circ}\text{C}$.

 Table 1. MSOP, QFN (LFCSP) 14-/16-/18-Bit PulSAR[®] ADCs

Type	100 kSPS	250 kSPS	400 kSPS to 500 kSPS	≥ 1000 kSPS	ADC Driver
18-Bit True Differential		AD7691	AD7690	AD7982 AD7984	ADA4941 ADA4841
16-Bit True Differential	AD7684	AD7687	AD7688 AD7693		ADA4941 ADA4841
16-Bit Pseudo Differential	AD7680 AD7683	AD7685 AD7694	AD7686	AD7980	ADA4841
14-Bit Pseudo Differential	AD7940	AD7942	AD7946		ADA4841

Rev. B

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REVISION HISTORY

7/13—Rev. A to Rev. B

Added Low Power Dissipation of 4 mW at 1 MSPS (VDD only) to Features Section.....	1
Changes to Power Dissipation; Table 3.....	4
Added EPAD Notation to Figure 5 and Table 6.....	7
Updated Outline Dimensions	24
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10/07—Rev. 0 to Rev. A

Changes to Table 1 and Layout.....	1
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3/07—Revision 0: Initial Version

SPECIFICATIONS

VDD = 2.5 V, VIO = 2.3 V to 5.5 V, REF = 5 V, TA = -40°C to +85°C, unless otherwise noted.

Table 2.

Parameter	Conditions	Min	Typ	Max	Unit
RESOLUTION		18			Bits
ANALOG INPUT					
Voltage Range	IN+ – IN–	–VREF		+VREF	V
Absolute Input Voltage	IN+, IN–	–0.1		VREF + 0.1	V
Common-Mode Input Range	IN+, IN–	VREF × 0.475	VREF × 0.5	VREF × 0.525	V
Analog Input CMRR	fIN = 450 kHz		67		dB
Leakage Current at 25°C	Acquisition phase		200		nA
Input Impedance		See the Analog Inputs section			
ACCURACY					
No Missing Codes		18			Bits
Differential Linearity Error		–0.85	±0.5	+1.5	LSB ¹
Integral Linearity Error		–2	±1	+2	LSB ¹
Transition Noise	REF = 5 V		1.05		LSB ¹
Gain Error, TMIN to TMAX ²		–0.023	+0.004	+0.023	% of FS
Gain Error Temperature Drift			±1		ppm/°C
Zero Error, TMIN to TMAX ²			±100	+700	μV
Zero Temperature Drift			0.5		ppm/°C
Power Supply Rejection Ratio	VDD = 2.5 V ± 5%		90		dB
THROUGHPUT					
Conversion Rate		0		1	MSPS
Transient Response	Full-scale step			290	ns
AC ACCURACY					
Dynamic Range	VREF = 5 V	97	99		dB ³
	VREF = 2.5 V		93		dB ³
Oversampled Dynamic Range ⁴	FO = 1 kSPS		129		dB ³
Signal-to-Noise	fIN = 1 kHz, VREF = 5 V, TA = 25°C	95.5	98		dB ³
	fIN = 1 kHz, VREF = 2.5 V, TA = 25°C		92.5		dB ³
Spurious-Free Dynamic Range	fIN = 10 kHz		–115		dB ³
Total Harmonic Distortion ⁵	fIN = 10 kHz		–120		dB ³
Signal-to-(Noise + Distortion)	fIN = 1 kHz, VREF = 5 V, TA = 25°C		97		dB ³

¹ LSB means least significant bit. With the ±5 V input range, 1 LSB is 38.15 μV.

² See Terminology section. These specifications include full temperature range variation but not the error contribution from the external reference.

³ All specifications expressed in decibels are referred to a full-scale input FSR and tested with an input signal at 0.5 dB below full scale, unless otherwise specified.

⁴ Dynamic range is obtained by oversampling the ADC running at a throughput FO of 1 MSPS followed by postdigital filtering with an output word rate of FO.

⁵ Tested fully in production at fIN = 1 kHz.

VDD = 2.5 V, VIO = 2.3 V to 5.5 V, REF = 5 V, T_A = -40°C to +85°C, unless otherwise noted.

Table 3.

Parameter	Conditions	Min	Typ	Max	Unit
REFERENCE					
Voltage Range		2.4		5.1	V
Load Current	1 MSPS, REF = 5 V		350		μA
SAMPLING DYNAMICS					
-3 dB Input Bandwidth			10		MHz
Aperture Delay	VDD = 2.5 V		2		ns
DIGITAL INPUTS					
Logic Levels					
V _{IL}	VIO > 3 V	-0.3		+0.3 × VIO	V
V _{IH}	VIO > 3 V	0.7 × VIO		VIO + 0.3	V
V _{IL}	VIO ≤ 3 V	-0.3		+0.1 × VIO	V
V _{IH}	VIO ≤ 3 V	0.9 × VIO		VIO + 0.3	V
I _{IL}		-1		+1	μA
I _{IH}		-1		+1	μA
DIGITAL OUTPUTS					
Data Format		Serial 18 bits, twos complement			
Pipeline Delay		Conversion results available immediately after completed conversion			
V _{OL}	I _{SINK} = +500 μA			0.4	V
V _{OH}	I _{SOURCE} = -500 μA	VIO - 0.3			V
POWER SUPPLIES					
VDD		2.375	2.5	2.625	V
VIO	Specified performance	2.3		5.5	V
VIO Range		1.8		5.5	V
Standby Current ^{1, 2}	VDD and VIO = 2.5 V, 25°C		0.35		μA
Power Dissipation					
Total	VDD = 2.625 V, V _{REF} = 5 V, VIO = 3 V		70	86	μW
	10 kSPS throughput		7	8.6	mW
	1 MSPS throughput		4		mW
VDD only			1.7		mW
REF only			1.3		mW
VIO only			7.0		nJ/sample
Energy per Conversion					
TEMPERATURE RANGE ³					
Specified Performance	T _{MIN} to T _{MAX}	-40		+85	°C

¹ With all digital inputs forced to VIO or GND as required.

² During acquisition phase.

³ Contact an Analog Devices, Inc. sales representative for the extended temperature range.

TIMING SPECIFICATIONS

T_A = -40°C to +85°C, V_{DD} = 2.37 V to 2.63 V, V_{IO} = 2.3 V to 5.5 V, unless otherwise noted.¹

Table 4.

Parameter	Symbol	Min	Typ	Max	Unit
Conversion Time: CNV Rising Edge to Data Available	t _{CONV}	500		710	ns
Acquisition Time	t _{ACQ}	290			ns
Time Between Conversions	t _{CYC}	1000			ns
CNV Pulse Width (CS Mode)	t _{CNVH}	10			ns
SCK Period (CS Mode)	t _{SCK}				
VIO Above 4.5 V		10.5			ns
VIO Above 3 V		12			ns
VIO Above 2.7 V		13			ns
VIO Above 2.3 V		15			ns
SCK Period (Chain Mode)	t _{SCK}				
VIO Above 4.5 V		11.5			ns
VIO Above 3 V		13			ns
VIO Above 2.7 V		14			ns
VIO Above 2.3 V		16			ns
SCK Low Time	t _{SCKL}	4.5			ns
SCK High Time	t _{SCKH}	4.5			ns
SCK Falling Edge to Data Remains Valid	t _{HSDO}	3			ns
SCK Falling Edge to Data Valid Delay	t _{DSDO}				
VIO Above 4.5 V				9.5	ns
VIO Above 3 V				11	ns
VIO Above 2.7 V				12	ns
VIO Above 2.3 V				14	ns
CNV or SDI Low to SDO D15 MSB Valid (CS Mode)	t _{EN}				
VIO Above 3 V				10	ns
VIO Above 2.3 V				15	ns
CNV or SDI High or Last SCK Falling Edge to SDO High Impedance (CS Mode)	t _{DIS}			20	ns
SDI Valid Setup Time from CNV Rising Edge	t _{SSDICNV}	5			ns
SDI Valid Hold Time from CNV Rising Edge (CS Mode)	t _{HSDICNV}	2			ns
SDI Valid Hold Time from CNV Rising Edge (Chain Mode)	t _{HSDICNV}	0			ns
SCK Valid Setup Time from CNV Rising Edge (Chain Mode)	t _{SSCKCNV}	5			ns
SCK Valid Hold Time from CNV Rising Edge (Chain Mode)	t _{HSCKCNV}	5			ns
SDI Valid Setup Time from SCK Falling Edge (Chain Mode)	t _{SSDISCK}	2			ns
SDI Valid Hold Time from SCK Falling Edge (Chain Mode)	t _{HSDISCK}	3			ns
SDI High to SDO High (Chain Mode with Busy Indicator)	t _{DSDOSDI}			15	ns

¹ See Figure 2 and Figure 3 for load conditions.

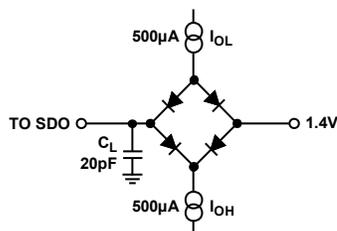
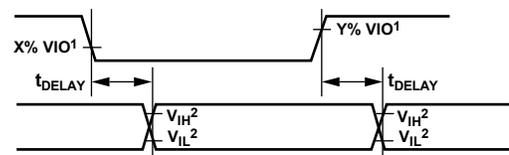


Figure 2. Load Circuit for Digital Interface Timing



¹FOR V_{IO} ≤ 3.0V, X = 90, AND Y = 10; FOR V_{IO} > 3.0V, X = 70, AND Y = 30.
²MINIMUM V_{IH} AND MAXIMUM V_{IL} USED. SEE DIGITAL INPUTS SPECIFICATIONS IN TABLE 3.

Figure 3. Voltage Levels for Timing

ABSOLUTE MAXIMUM RATINGS

Table 5.

Parameter	Rating
Analog Inputs IN+, IN- to GND ¹	-0.3 V to $V_{REF} + 0.3$ V or ± 130 mA
Supply Voltage REF, VIO to GND	-0.3 V to +6.0 V
VDD to GND	-0.3 V to +3.0 V
VDD to VIO	+3 V to -6 V
Digital Inputs to GND	-0.3 V to VIO + 0.3 V
Digital Outputs to GND	-0.3 V to VIO + 0.3 V
Storage Temperature Range	-65°C to +150°C
Junction Temperature	150°C
θ_{JA} Thermal Impedance	
10-Lead MSOP	200°C/W
10-Lead QFN (LFCSP_WD)	48.7°C/W
θ_{JC} Thermal Impedance	
10-Lead MSOP	44°C/W
10-Lead QFN (LFCSP_WD)	2.96°C/W
Lead Temperatures	
Vapor Phase (60 sec)	215°C
Infrared (15 sec)	220°C

¹ See the Analog Inputs section for an explanation of IN+ and IN-.

Stresses above those listed under Absolute Maximum Ratings may cause permanent damage to the device. This is a stress rating only; functional operation of the device at these or any other conditions above those indicated in the operational section of this specification is not implied. Exposure to absolute maximum rating conditions for extended periods may affect device reliability.

ESD CAUTION



ESD (electrostatic discharge) sensitive device. Charged devices and circuit boards can discharge without detection. Although this product features patented or proprietary protection circuitry, damage may occur on devices subjected to high energy ESD. Therefore, proper ESD precautions should be taken to avoid performance degradation or loss of functionality.

PIN CONFIGURATIONS AND FUNCTION DESCRIPTIONS

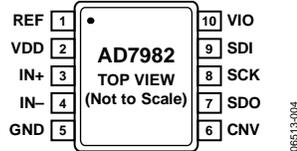
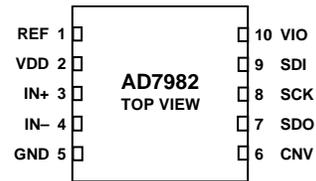


Figure 4. 10-Lead MSOP Pin Configuration



NOTES

1. THE EXPOSED PAD SHOULD BE CONNECTED TO GND. THIS CONNECTION IS NOT REQUIRED TO MEET THE ELECTRICAL PERFORMANCES.

Figure 5. 10-Lead QFN (LFCSP) Pin Configuration

Table 6. Pin Function Descriptions

Pin No.	Mnemonic	Type ¹	Description
1	REF	AI	Reference Input Voltage. The REF range is 2.4 V to 5.1 V. This pin is referred to the GND pin and should be decoupled closely to the GND pin with a 10 μ F capacitor.
2	VDD	P	Power Supply.
3	IN+	AI	Differential Positive Analog Input.
4	IN-	AI	Differential Negative Analog Input.
5	GND	P	Power Supply Ground.
6	CNV	DI	Convert Input. This input has multiple functions. On its leading edge, it initiates the conversions and selects the interface mode of the part: chain mode or \overline{CS} mode. In \overline{CS} mode, the SDO pin is enabled when CNV is low. In chain mode, the data should be read when CNV is high.
7	SDO	DO	Serial Data Output. The conversion result is output on this pin. It is synchronized to SCK.
8	SCK	DI	Serial Data Clock Input. When the part is selected, the conversion result is shifted out by this clock.
9	SDI	DI	Serial Data Input. This input provides multiple features. It selects the interface mode of the ADC as follows: Chain mode is selected if SDI is low during the CNV rising edge. In this mode, SDI is used as a data input to daisy-chain the conversion results of two or more ADCs onto a single SDO line. The digital data level on SDI is output on SDO with a delay of 18 SCK cycles. \overline{CS} mode is selected if SDI is high during the CNV rising edge. In this mode, either SDI or CNV can enable the serial output signals when low. If SDI or CNV is low when the conversion is complete, the busy indicator feature is enabled.
10	VIO EPAD	P	Input/Output Interface Digital Power. Nominally at the same supply as the host interface (1.8 V, 2.5 V, 3 V, or 5 V). Exposed Pad. For the lead frame chip scale package (LFCSP), the exposed pad should be connected to GND. this connection is not required to meet the electrical performances.

¹AI = analog input, DI = digital input, DO = digital output, and P = power.

TERMINOLOGY

Integral Nonlinearity Error (INL)

INL refers to the deviation of each individual code from a line drawn from negative full scale through positive full scale. The point used as negative full scale occurs ½ LSB before the first code transition. Positive full scale is defined as a level 1½ LSB beyond the last code transition. The deviation is measured from the middle of each code to the true straight line (see Figure 22).

Differential Nonlinearity Error (DNL)

In an ideal ADC, code transitions are 1 LSB apart. DNL is the maximum deviation from this ideal value. It is often specified in terms of resolution for which no missing codes are guaranteed.

Zero Error

Zero error is the difference between the ideal midscale voltage, that is, 0 V, from the actual voltage producing the midscale output code, that is, 0 LSB.

Gain Error

The first transition (from 100 ... 00 to 100 ... 01) should occur at a level ½ LSB above nominal negative full scale (–4.999981 V for the ±5 V range). The last transition (from 011 ... 10 to 011 ... 11) should occur for an analog voltage 1½ LSB below the nominal full scale (+4.999943 V for the ±5 V range). The gain error is the deviation of the difference between the actual level of the last transition and the actual level of the first transition from the difference between the ideal levels.

Spurious-Free Dynamic Range (SFDR)

SFDR is the difference, in decibels (dB), between the rms amplitude of the input signal and the peak spurious signal.

Effective Number of Bits (ENOB)

ENOB is a measurement of the resolution with a sine wave input. It is related to SINAD as follows

$$ENOB = (SINAD_{dB} - 1.76)/6.02$$

and is expressed in bits.

Noise-Free Code Resolution

Noise-free code resolution is the number of bits beyond which it is impossible to distinctly resolve individual codes. It is calculated as

$$Noise\text{-Free Code Resolution} = \log_2(2^N/Peak\text{-to-Peak Noise})$$

and is expressed in bits.

Effective Resolution

Effective resolution is calculated as

$$Effective\ Resolution = \log_2(2^N/RMS\ Input\ Noise)$$

and is expressed in bits.

Total Harmonic Distortion (THD)

THD is the ratio of the rms sum of the first five harmonic components to the rms value of a full-scale input signal and is expressed in decibels.

Dynamic Range

Dynamic range is the ratio of the rms value of the full scale to the total rms noise measured with the inputs shorted together. The value for dynamic range is expressed in decibels. It is measured with a signal at –60 dBFS so that it includes all noise sources and DNL artifacts.

Signal-to-Noise Ratio (SNR)

SNR is the ratio of the rms value of the actual input signal to the rms sum of all other spectral components below the Nyquist frequency, excluding harmonics and dc. The value for SNR is expressed in decibels.

Signal-to-(Noise + Distortion) Ratio (SINAD)

SINAD is the ratio of the rms value of the actual input signal to the rms sum of all other spectral components that are less than the Nyquist frequency, including harmonics but excluding dc. The value of SINAD is expressed in decibels.

Aperture Delay

Aperture delay is the measure of the acquisition performance and is the time between the rising edge of the CNV input and when the input signal is held for a conversion.

Transient Response

Transient response is the time required for the ADC to accurately acquire its input after a full-scale step function is applied.

TYPICAL PERFORMANCE CHARACTERISTICS

VDD = 2.5 V, REF = 5.0 V, VIO = 3.3 V.

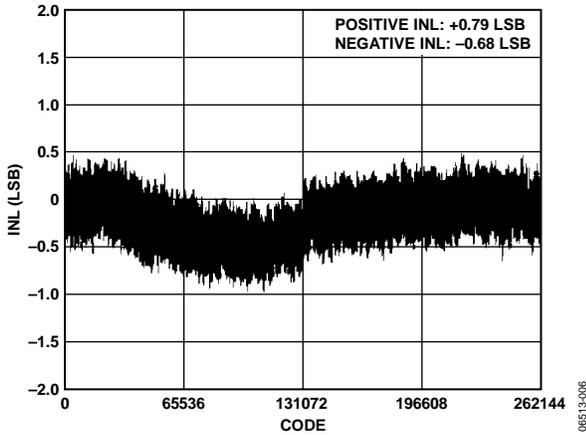


Figure 6. Integral Nonlinearity vs. Code

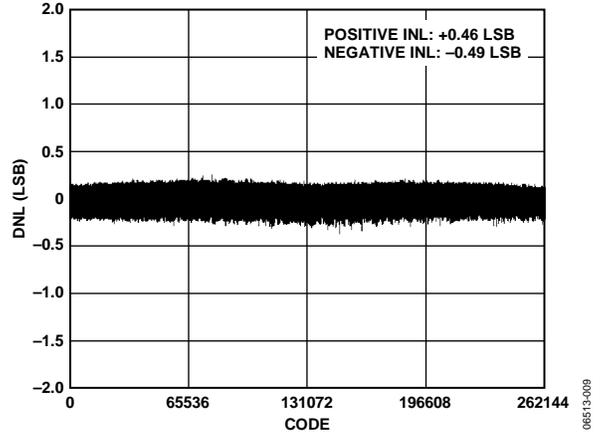


Figure 9. Differential Nonlinearity vs. Code

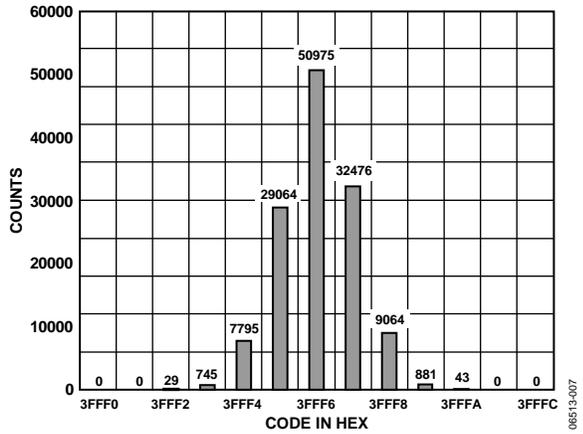


Figure 7. Histogram of a DC Input at the Code Center

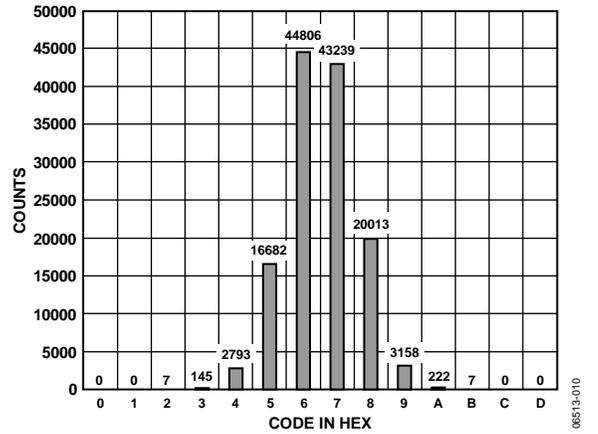


Figure 10. Histogram of a DC Input at the Code Transition

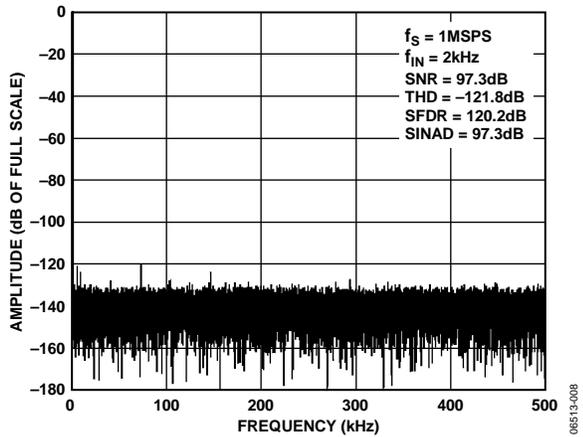


Figure 8. FFT Plot

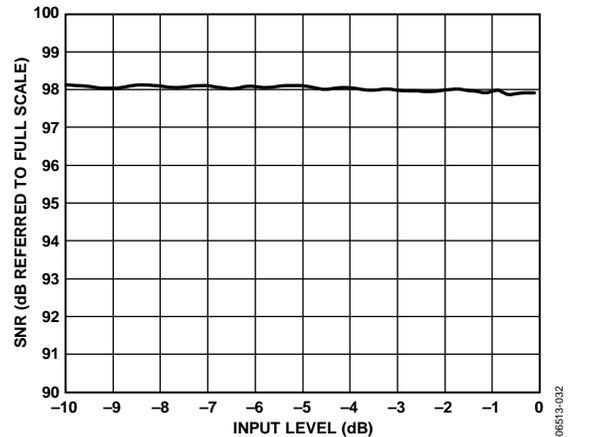


Figure 11. SNR vs. Input Level

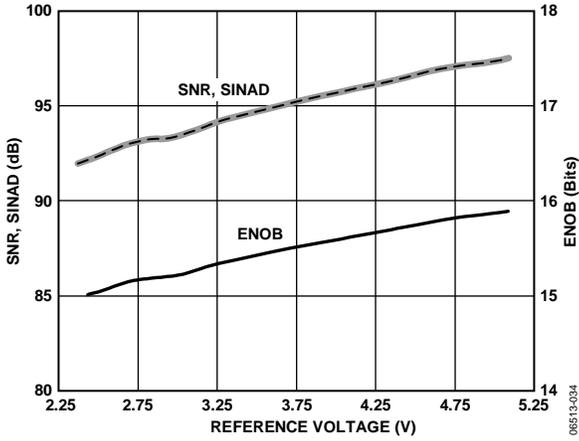


Figure 12. SNR, SINAD, and ENOB vs. Reference Voltage

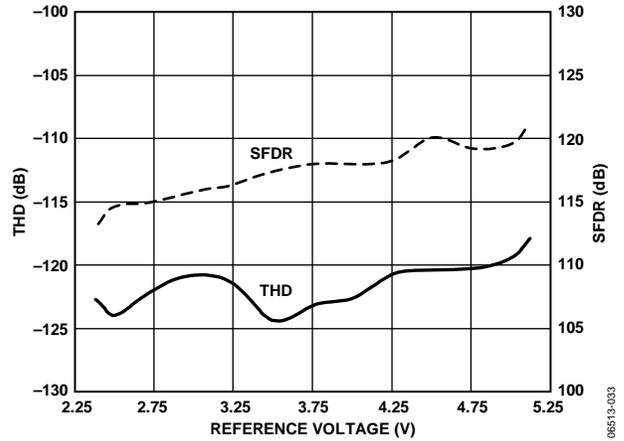


Figure 15. THD, SFDR vs. Reference Voltage

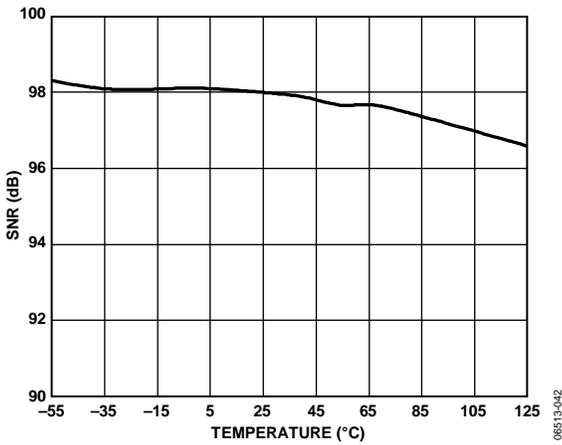


Figure 13. SNR vs. Temperature

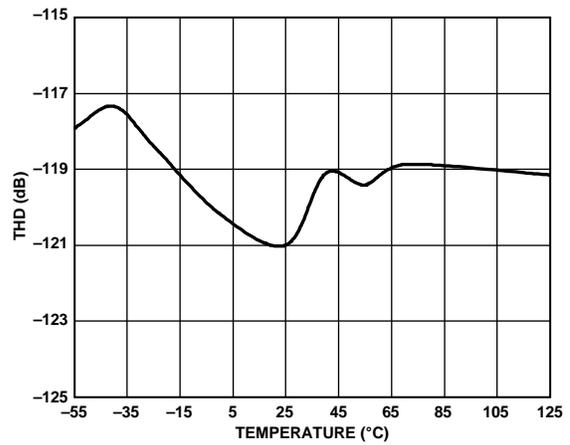


Figure 16. THD vs. Temperature

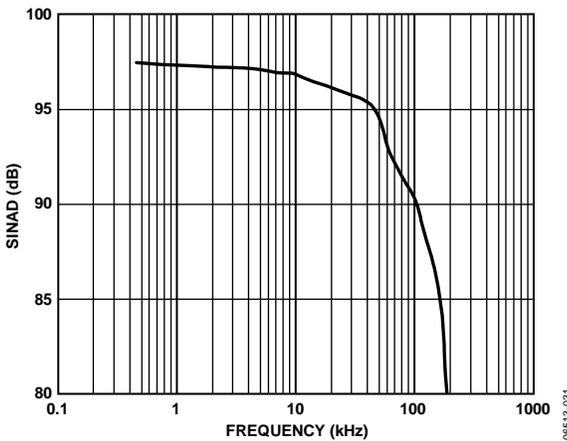


Figure 14. SINAD vs. Frequency

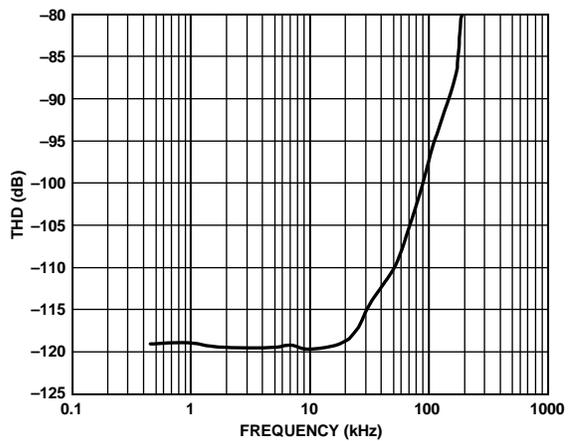


Figure 17. THD vs. Frequency

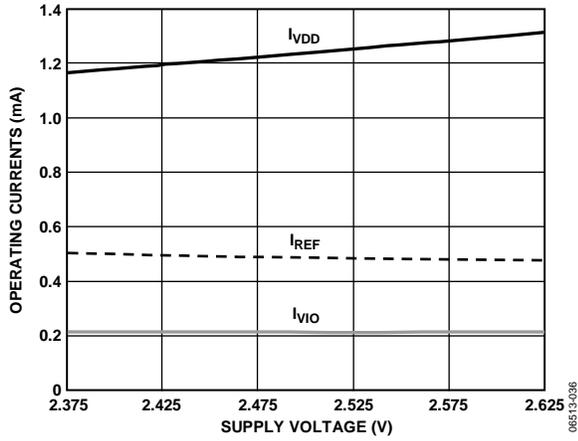


Figure 18. Operating Currents vs. Supply Voltage

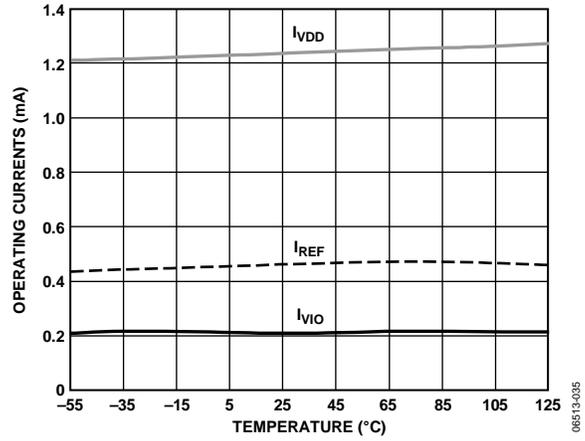


Figure 20. Operating Currents vs. Temperature

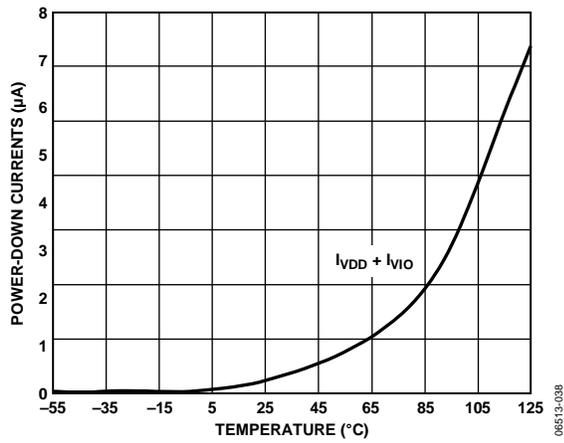


Figure 19. Power-Down Currents vs. Temperature

THEORY OF OPERATION

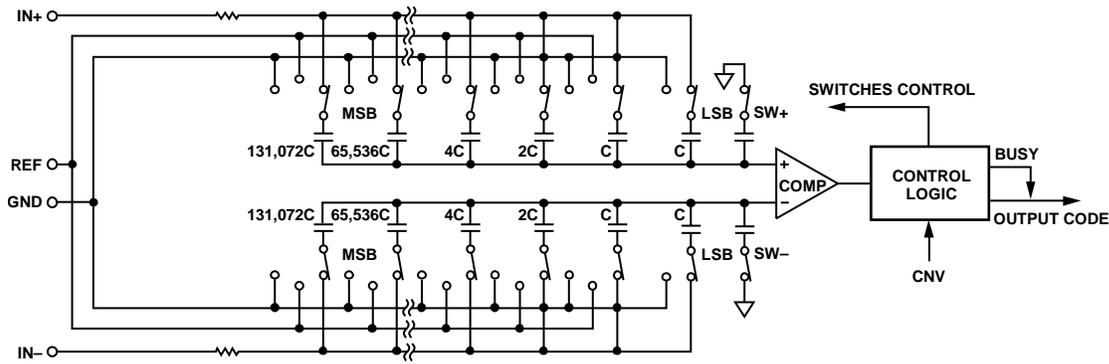


Figure 21. ADC Simplified Schematic

08513-011

CIRCUIT INFORMATION

The AD7982 is a fast, low power, single-supply, precise, 18-bit ADC using a successive approximation architecture.

The AD7982 is capable of converting 1,000,000 samples per second (1 MSPS) and powers down between conversions. When operating at 10 kSPS, for example, it typically consumes 70 μ W, making it ideal for battery-powered applications.

The AD7982 provides the user with an on-chip track-and-hold and does not exhibit any pipeline delay or latency, making it ideal for multiple multiplexed channel applications.

The AD7982 can be interfaced to any 1.8 V to 5 V digital logic family. It is available in a 10-lead MSOP or a tiny 10-lead QFN (LFCSP) that allows space savings and flexible configurations.

It is pin-for-pin-compatible with the 16-bit [AD7980](#).

CONVERTER OPERATION

The AD7982 is a successive approximation ADC based on a charge redistribution DAC. Figure 21 shows the simplified schematic of the ADC. The capacitive DAC consists of two identical arrays of 18 binary-weighted capacitors, which are connected to the two comparator inputs.

During the acquisition phase, terminals of the array tied to the input of the comparator are connected to GND via SW+ and SW-. All independent switches are connected to the analog inputs. Therefore, the capacitor arrays are used as sampling capacitors and acquire the analog signal on the IN+ and IN- inputs. When the acquisition phase is complete and the CNV input goes high, a conversion phase is initiated. When the conversion phase begins, SW+ and SW- are opened first. The two capacitor arrays are then disconnected from the inputs and connected to the GND input. Therefore, the differential voltage between the inputs IN+ and IN- captured at the end of the acquisition phase is applied to the comparator inputs, causing the comparator to become unbalanced. By switching each element of the capacitor array between GND and REF, the comparator input varies by binary-weighted voltage steps ($V_{REF}/2$, $V_{REF}/4$... $V_{REF}/262,144$). The control logic toggles these switches, starting with the MSB, to bring the comparator back into a balanced condition. After the completion of this process, the part returns to the acquisition phase, and the control logic generates the ADC output code and a busy signal indicator.

Because the AD7982 has an on-board conversion clock, the serial clock, SCK, is not required for the conversion process.

Transfer Functions

The ideal transfer characteristic for the AD7982 is shown in Figure 22 and Table 7.

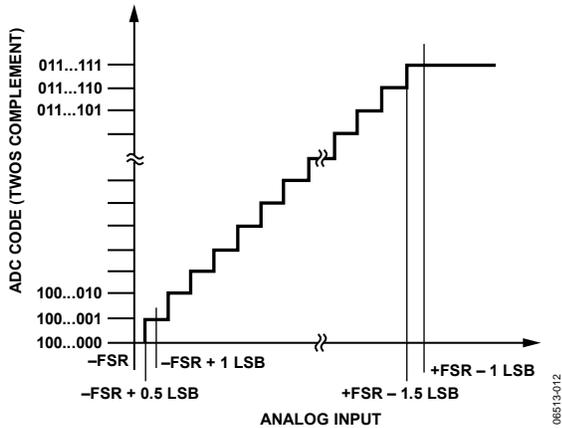


Figure 22. ADC Ideal Transfer Function

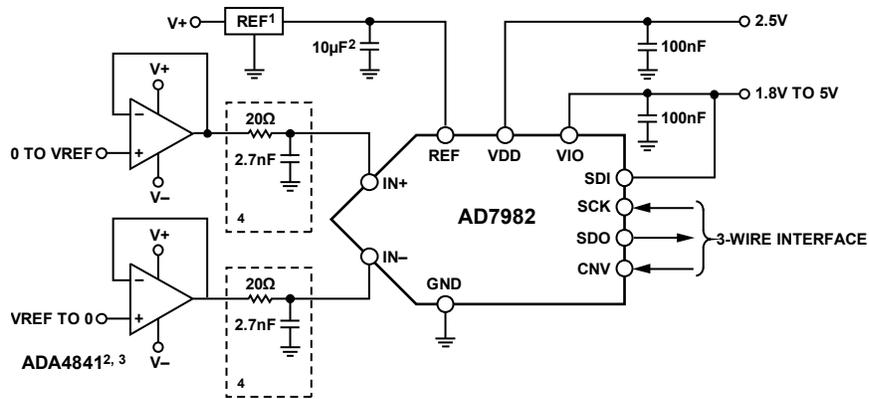
Table 7. Output Codes and Ideal Input Voltages

Description	Analog Input $V_{REF} = 5V$	Digital Output Code (Hex)
FSR - 1 LSB	+4.999962 V	0x1FFFF ¹
Midscale + 1 LSB	+38.15 μ V	0x00001
Midscale	0 V	0x00000
Midscale - 1 LSB	-38.15 μ V	0x3FFFF
-FSR + 1 LSB	-4.999962 V	0x20001
-FSR	-5 V	0x20000 ²

¹ This is also the code for an overranged analog input ($V_{IN+} - V_{IN-}$ above $V_{REF} - V_{GND}$).
² This is also the code for an underranged analog input ($V_{IN+} - V_{IN-}$ below V_{GND}).

TYPICAL CONNECTION DIAGRAM

Figure 23 shows an example of the recommended connection diagram for the AD7982 when multiple supplies are available.



- NOTES**
- ¹SEE VOLTAGE REFERENCE INPUT SECTION FOR REFERENCE SELECTION.
 - ² C_{REF} IS USUALLY A 10 μ F CERAMIC CAPACITOR (X5R).
SEE RECOMMENDED LAYOUT FIGURE 41 AND FIGURE 42.
 - ³SEE DRIVER AMPLIFIER CHOICE SECTION.
 - ⁴OPTIONAL FILTER. SEE ANALOG INPUT SECTION.

Figure 23. Typical Application Diagram with Multiple Supplies

ANALOG INPUTS

Figure 24 shows an equivalent circuit of the input structure of the AD7982.

The two diodes, D1 and D2, provide ESD protection for the analog inputs, IN+ and IN-. Care must be taken to ensure that the analog input signal does not exceed the reference input voltage (REF) by more than 0.3 V. If the analog input signal exceeds this level, the diodes become forward biased and start conducting current. These diodes can handle a forward-biased current of 130 mA maximum. However, if the supplies of the input buffer (for example, the supplies of the ADA4841 in Figure 23) are different from those of the REF, the analog input signal may eventually exceed the supply rails by more than 0.3 V. In such a case (for example, an input buffer with a short-circuit), the current limitation can be used to protect the part.

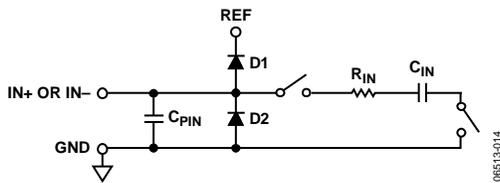


Figure 24. Equivalent Analog Input Circuit

The analog input structure allows the sampling of the true differential signal between IN+ and IN-. By using these differential inputs, signals common to both inputs are rejected.

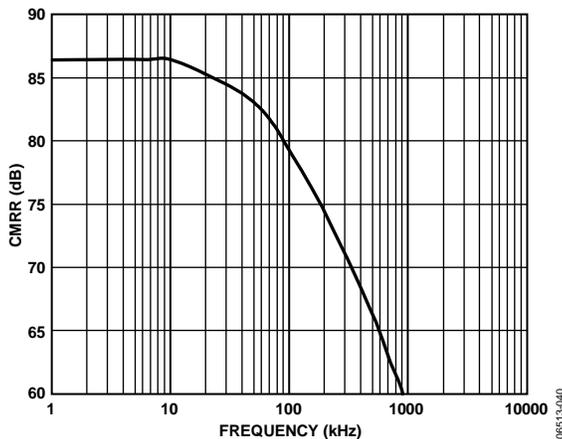


Figure 25. Analog Input CMRR vs. Frequency

During the acquisition phase, the impedance of the analog inputs (IN+ or IN-) can be modeled as a parallel combination of Capacitor C_{PIN} and the network formed by the series connection of R_{IN} and C_{IN} . C_{PIN} is primarily the pin capacitance. R_{IN} is typically 400 Ω and is a lumped component composed of serial resistors and the on resistance of the switches. C_{IN} is typically 30 pF and is mainly the ADC sampling capacitor.

During the sampling phase, where the switches are closed, the input impedance is limited to C_{PIN} . R_{IN} and C_{IN} make a 1-pole, low-pass filter that reduces undesirable aliasing effects and limits noise.

When the source impedance of the driving circuit is low, the AD7982 can be driven directly. Large source impedances significantly affect the ac performance, especially THD. The dc performances are less sensitive to the input impedance. The maximum source impedance depends on the amount of THD that can be tolerated. The THD degrades as a function of the source impedance and the maximum input frequency.

DRIVER AMPLIFIER CHOICE

Although the AD7982 is easy to drive, the driver amplifier must meet the following requirements:

- The noise generated by the driver amplifier must be kept as low as possible to preserve the SNR and transition noise performance of the AD7982. The noise from the driver is filtered by the AD7982 analog input circuit's 1-pole, low-pass filter made by R_{IN} and C_{IN} or by the external filter, if one is used. Because the typical noise of the AD7982 is 40 μ V rms, the SNR degradation due to the amplifier is

$$SNR_{LOSS} = 20 \log \left(\frac{40}{\sqrt{40^2 + \frac{\pi}{2} f_{-3dB} (Ne_N)^2}} \right)$$

where:

f_{-3dB} is the input bandwidth, in megahertz, of the AD7982 (10 MHz) or the cutoff frequency of the input filter, if one is used.

N is the noise gain of the amplifier (for example, 1 in buffer configuration).

e_N is the equivalent input noise voltage of the op amp, in nV/\sqrt{Hz} .

- For ac applications, the driver should have a THD performance commensurate with the AD7982.
- For multichannel multiplexed applications, the driver amplifier and the AD7982 analog input circuit must settle for a full-scale step onto the capacitor array at an 18-bit level (0.0004%, 4 ppm). In the data sheet of the amplifier, settling at 0.1% to 0.01% is more commonly specified. This may differ significantly from the settling time at an 18-bit level and should be verified prior to driver selection.

Table 8. Recommended Driver Amplifiers

Amplifier	Typical Application
ADA4941-1	Very low noise, low power, single to differential
ADA4841	Very low noise, small, and low power
AD8021	Very low noise and high frequency
AD8022	Low noise and high frequency
OP184	Low power, low noise, and low frequency
AD8655	5 V single supply, low noise
AD8605, AD8615	5 V single supply, low power

SINGLE-TO-DIFFERENTIAL DRIVER

For applications using a single-ended analog signal, either bipolar or unipolar, the ADA4941 single-ended-to-differential driver allows for a differential input to the part. The schematic is shown in Figure 26.

R1 and R2 set the attenuation ratio between the input range and the ADC range (V_{REF}). R1, R2, and C_F are chosen depending on the desired input resistance, signal bandwidth, antialiasing, and noise contribution. For example, for the ± 10 V range with a 4 k Ω impedance, R2 = 1 k Ω and R1 = 4 k Ω .

R3 and R4 set the common mode on the IN $-$ input, and R5 and R6 set the common mode on the IN $+$ input of the ADC. The common mode should be close to $V_{REF}/2$. For example, for the ± 10 V range with a single supply, R3 = 8.45 k Ω , R4 = 11.8 k Ω , R5 = 10.5 k Ω , and R6 = 9.76 k Ω .

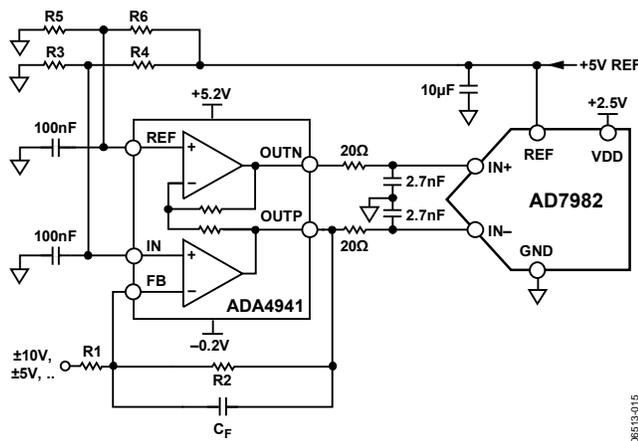


Figure 26. Single-Ended-to-Differential Driver Circuit

VOLTAGE REFERENCE INPUT

The AD7982 voltage reference input, REF, has a dynamic input impedance and should therefore be driven by a low impedance source with efficient decoupling between the REF and GND pins, as explained in the Layout section.

When REF is driven by a very low impedance source (for example, a reference buffer using the AD8031 or the AD8605), a 10 μ F (X5R, 0805 size) ceramic chip capacitor is appropriate for optimum performance.

If an unbuffered reference voltage is used, the decoupling value depends on the reference used. For instance, a 22 μ F (X5R, 1206 size) ceramic chip capacitor is appropriate for optimum performance using a low temperature drift ADR43x reference.

If desired, a reference decoupling capacitor with values as small as 2.2 μ F can be used with a minimal impact on performance, especially DNL.

Regardless, there is no need for an additional lower value ceramic decoupling capacitor (for example, 100 nF) between the REF and GND pins.

POWER SUPPLY

The AD7982 uses two power supply pins: a core supply (VDD) and a digital input/output interface supply (VIO). VIO allows direct interface with any logic between 1.8 V and 5.5 V. To reduce the number of supplies needed, VIO and VDD can be tied together. The AD7982 is independent of power supply sequencing between VIO and VDD. Additionally, it is very insensitive to power supply variations over a wide frequency range, as shown in Figure 27.

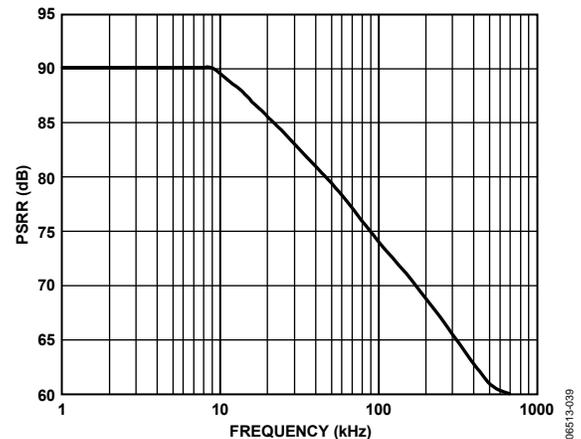


Figure 27. PSRR vs. Frequency

To ensure optimum performance, VDD should be roughly half of REF, the voltage reference input. For example, if REF is 5.0 V, VDD should be set to 2.5 V ($\pm 5\%$).

The AD7982 powers down automatically at the end of each conversion phase; therefore, the power scales linearly with the sampling rate. This makes the part ideal for low sampling rates (even of a few hertz) and low battery-powered applications.

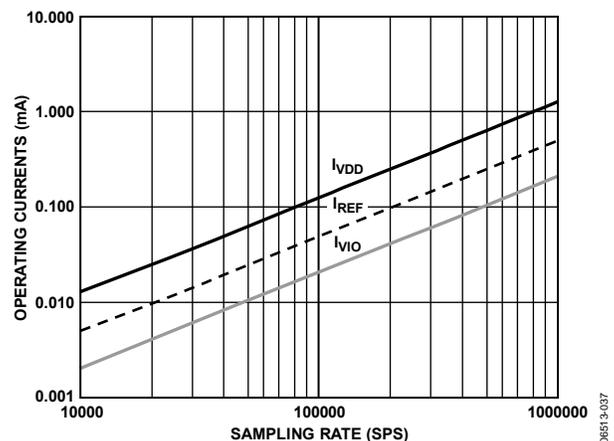


Figure 28. Operating Currents vs. Sampling Rate

DIGITAL INTERFACE

Although the AD7982 has a reduced number of pins, it offers flexibility in its serial interface modes.

When in \overline{CS} mode, the AD7982 is compatible with SPI, QSPI, digital hosts, and DSPs. In this mode, the AD7982 can use either a 3-wire or 4-wire interface. A 3-wire interface using the CNV, SCK, and SDO signals minimizes wiring connections useful, for instance, in isolated applications. A 4-wire interface using the SDI, CNV, SCK, and SDO signals allows CNV, which initiates the conversions, to be independent of the readback timing (SDI). This is useful in low jitter sampling or simultaneous sampling applications.

When in chain mode, the AD7982 provides a daisy-chain feature using the SDI input for cascading multiple ADCs on a single data line similar to a shift register.

The mode in which the part operates depends on the SDI level when the CNV rising edge occurs. The \overline{CS} mode is selected if SDI is high, and the chain mode is selected if SDI is low. The SDI hold time is such that when SDI and CNV are connected together, the chain mode is always selected.

In either mode, the AD7982 offers the option of forcing a start bit in front of the data bits. This start bit can be used as a busy signal indicator to interrupt the digital host and trigger the data reading. Otherwise, without a busy indicator, the user must timeout the maximum conversion time prior to readback.

The busy indicator feature is enabled

- In the \overline{CS} mode if CNV or SDI is low when the ADC conversion ends (see Figure 32 and Figure 36).
- In the chain mode if SCK is high during the CNV rising edge (see Figure 40).

\overline{CS} MODE, 3-WIRE WITHOUT BUSY INDICATOR

This mode is usually used when a single AD7982 is connected to an SPI-compatible digital host. The connection diagram is shown in Figure 29, and the corresponding timing is given in Figure 30.

With SDI tied to VIO, a rising edge on CNV initiates a conversion, selects the \overline{CS} mode, and forces SDO to high impedance. Once a conversion is initiated, it continues until completion irrespective of the state of CNV. This can be useful, for instance, to bring CNV low to select other SPI devices, such as analog multiplexers; however, CNV must be returned high before the minimum conversion time elapses and then held

high for the maximum possible conversion time to avoid the generation of the busy signal indicator. When the conversion is complete, the AD7982 enters the acquisition phase and powers down. When CNV goes low, the MSB is output onto SDO. The remaining data bits are clocked by subsequent SCK falling edges. The data is valid on both SCK edges. Although the rising edge can be used to capture the data, a digital host using the SCK falling edge allows a faster reading rate, provided it has an acceptable hold time. After the 18th SCK falling edge or when CNV goes high (whichever occurs first), SDO returns to high impedance.

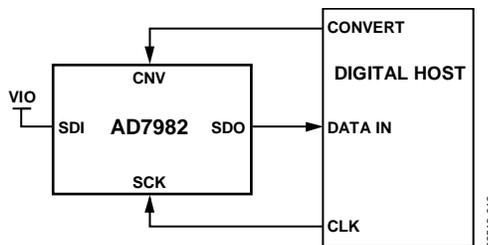


Figure 29. \overline{CS} Mode, 3-Wire Without Busy Indicator Connection Diagram (SDI High)

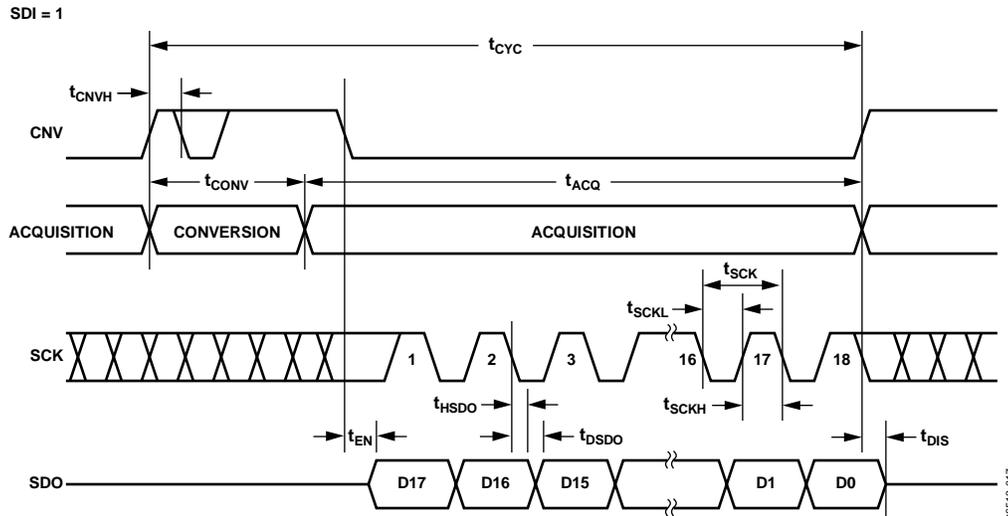


Figure 30. \overline{CS} Mode, 3-Wire Without Busy Indicator Serial Interface Timing (SDI High)

$\overline{\text{CS}}$ MODE, 3-WIRE WITH BUSY INDICATOR

This mode is usually used when a single AD7982 is connected to an SPI-compatible digital host having an interrupt input.

The connection diagram is shown in Figure 31, and the corresponding timing is given in Figure 32.

With SDI tied to VIO, a rising edge on CNV initiates a conversion, selects the $\overline{\text{CS}}$ mode, and forces SDO to high impedance. SDO is maintained in high impedance until the completion of the conversion irrespective of the state of CNV. Prior to the minimum conversion time, CNV can be used to select other SPI devices, such as analog multiplexers, but CNV must be returned low before the minimum conversion time elapses and then held low for the maximum possible conversion time to guarantee the generation of the busy signal indicator.

When the conversion is complete, SDO goes from high impedance to low impedance. With a pull-up on the SDO line, this transition can be used as an interrupt signal to initiate the data reading controlled by the digital host. The AD7982 then enters the acquisition phase and powers down. The data bits are then clocked out, MSB first, by subsequent SCK falling edges. The data is valid on both SCK edges. Although the rising edge can be used to capture the data, a digital host using the SCK falling edge allows a faster reading rate, provided it has an acceptable hold time. After the optional 19th SCK falling edge or when CNV goes high (whichever occurs first), SDO returns to high impedance.

If multiple AD7982s are selected at the same time, the SDO output pin handles this contention without damage or induced latch-up. Meanwhile, it is recommended to keep this contention as short as possible to limit extra power dissipation.

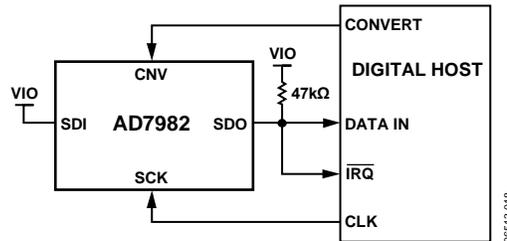


Figure 31. $\overline{\text{CS}}$ Mode, 3-Wire with Busy Indicator Connection Diagram (SDI High)

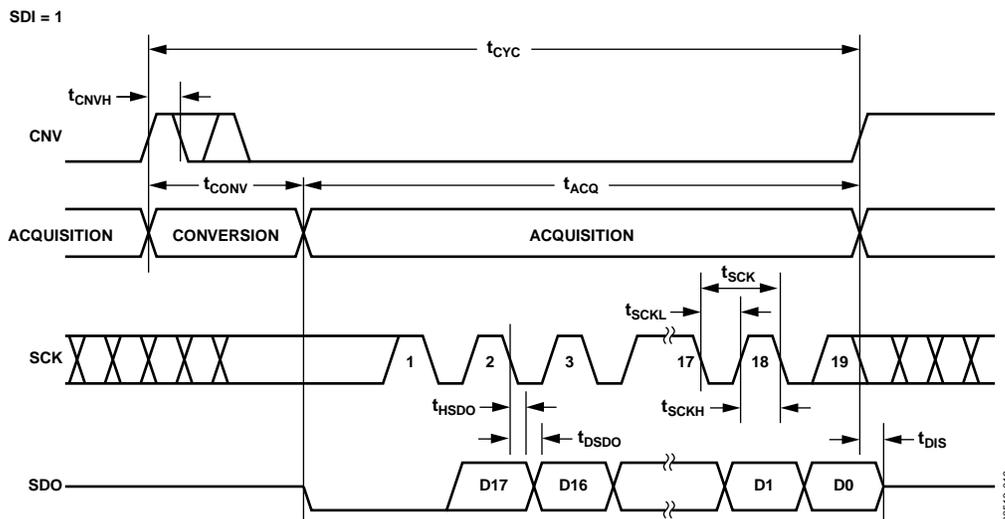


Figure 32. $\overline{\text{CS}}$ Mode, 3-Wire with Busy Indicator Serial Interface Timing (SDI High)

$\overline{\text{CS}}$ MODE, 4-WIRE WITHOUT BUSY INDICATOR

This mode is usually used when multiple AD7982s are connected to an SPI-compatible digital host.

A connection diagram example using two AD7982s is shown in Figure 33, and the corresponding timing is given in Figure 34.

With SDI high, a rising edge on CNV initiates a conversion, selects the $\overline{\text{CS}}$ mode, and forces SDO to high impedance. In this mode, CNV must be held high during the conversion phase and the subsequent data readback. (If SDI and CNV are low, SDO is driven low.) Prior to the minimum conversion time, SDI can be used to select other SPI devices, such as analog multiplexers, but SDI must be returned high before the minimum conversion

time elapses and then held high for the maximum possible conversion time to avoid the generation of the busy signal indicator. When the conversion is complete, the AD7982 enters the acquisition phase and powers down. Each ADC result can be read by bringing its SDI input low, which consequently outputs the MSB onto SDO. The remaining data bits are then clocked by subsequent SCK falling edges. The data is valid on both SCK edges. Although the rising edge can be used to capture the data, a digital host using the SCK falling edge allows a faster reading rate, provided it has an acceptable hold time. After the 18th SCK falling edge or when SDI goes high (whichever occurs first), SDO returns to high impedance and another AD7982 can be read.

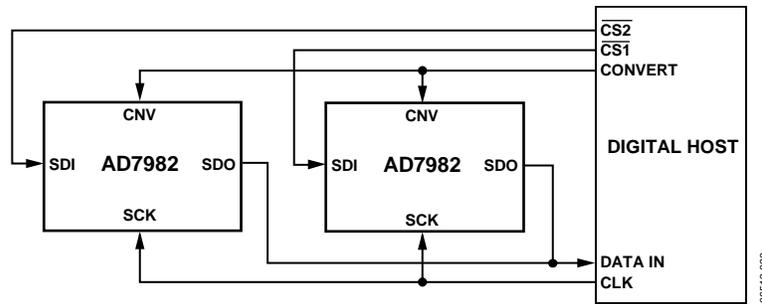


Figure 33. $\overline{\text{CS}}$ Mode, 4-Wire Without Busy Indicator Connection Diagram

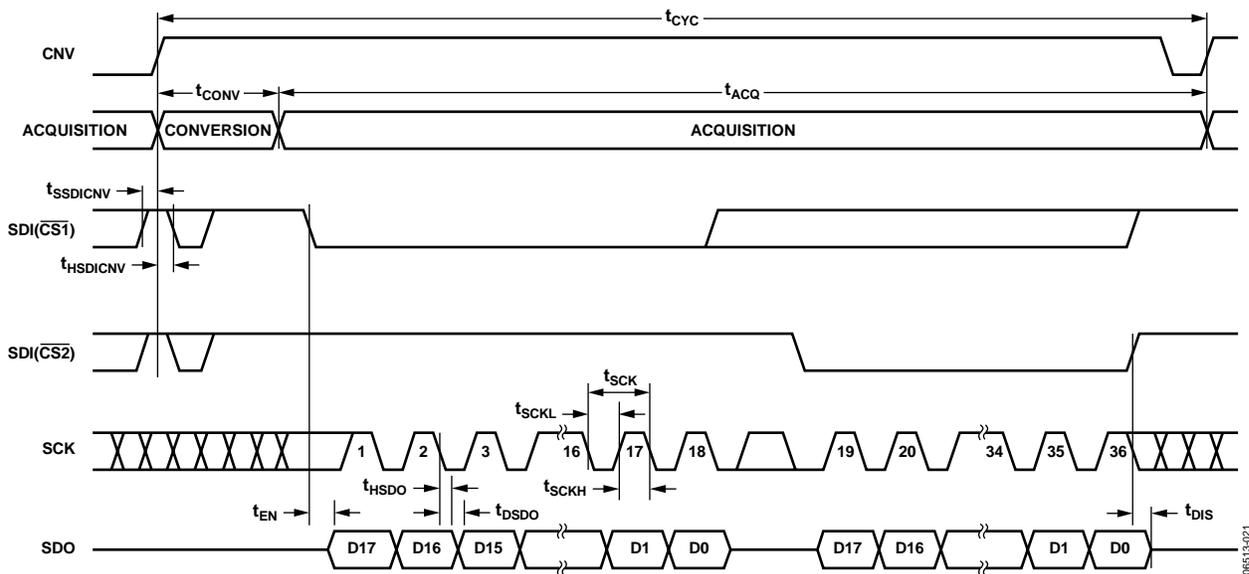


Figure 34. $\overline{\text{CS}}$ Mode, 4-Wire Without Busy Indicator Serial Interface Timing

CS MODE, 4-WIRE WITH BUSY INDICATOR

This mode is usually used when a single AD7982 is connected to an SPI-compatible digital host with an interrupt input and when it is desired to keep CNV, which is used to sample the analog input, independent of the signal used to select the data reading. This independence is particularly important in applications where low jitter on CNV is desired.

The connection diagram is shown in Figure 35, and the corresponding timing is given in Figure 36.

With SDI high, a rising edge on CNV initiates a conversion, selects the CS mode, and forces SDO to high impedance. In this mode, CNV must be held high during the conversion phase and the subsequent data readback. (If SDI and CNV are low, SDO is driven low.) Prior to the minimum conversion time, SDI can be

used to select other SPI devices, such as analog multiplexers, but SDI must be returned low before the minimum conversion time elapses and then held low for the maximum possible conversion time to guarantee the generation of the busy signal indicator. When the conversion is complete, SDO goes from high impedance to low impedance. With a pull-up on the SDO line, this transition can be used as an interrupt signal to initiate the data readback controlled by the digital host. The AD7982 then enters the acquisition phase and powers down. The data bits are then clocked out, MSB first, by subsequent SCK falling edges. The data is valid on both SCK edges. Although the rising edge can be used to capture the data, a digital host using the SCK falling edge allows a faster reading rate, provided it has an acceptable hold time. After the optional 19th SCK falling edge or SDI going high (whichever occurs first), SDO returns to high impedance.

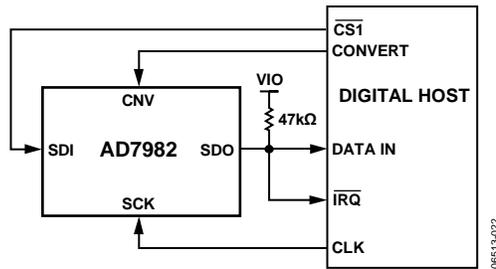


Figure 35. CS Mode, 4-Wire with Busy Indicator Connection Diagram

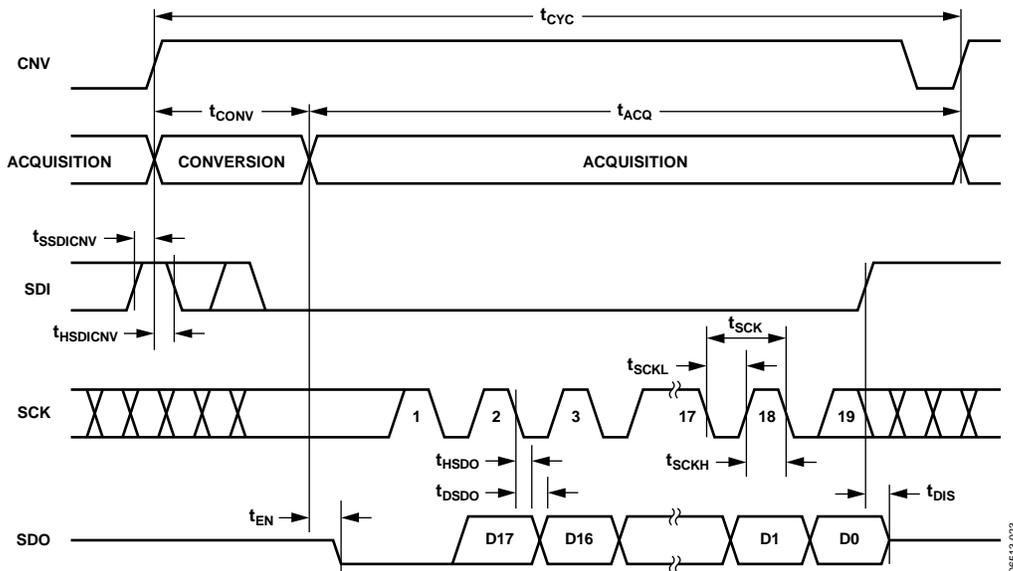


Figure 36. CS Mode, 4-Wire with Busy Indicator Serial Interface Timing

CHAIN MODE WITHOUT BUSY INDICATOR

This mode can be used to daisy-chain multiple AD7982s on a 3-wire serial interface. This feature is useful for reducing component count and wiring connections, for example, in isolated multiconverter applications or for systems with a limited interfacing capacity. Data readback is analogous to clocking a shift register.

A connection diagram example using two AD7982s is shown in Figure 37, and the corresponding timing is given in Figure 38.

When SDI and CNV are low, SDO is driven low. With SCK low, a rising edge on CNV initiates a conversion, selects the chain mode, and disables the busy indicator. In this mode, CNV is

held high during the conversion phase and the subsequent data readback. When the conversion is complete, the MSB is output onto SDO and the AD7982 enters the acquisition phase and powers down. The remaining data bits stored in the internal shift register are clocked by subsequent SCK falling edges. For each ADC, SDI feeds the input of the internal shift register and is clocked by the SCK falling edge. Each ADC in the chain outputs its data MSB first, and $18 \times N$ clocks are required to read back the N ADCs. The data is valid on both SCK edges. Although the rising edge can be used to capture the data, a digital host using the SCK falling edge allows a faster reading rate and consequently more AD7982s in the chain, provided the digital host has an acceptable hold time. The maximum conversion rate may be reduced due to the total readback time.

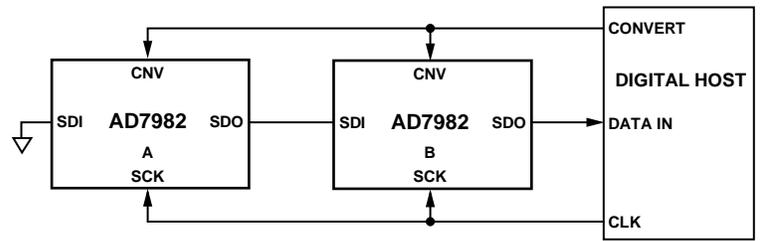


Figure 37. Chain Mode Without Busy Indicator Connection Diagram

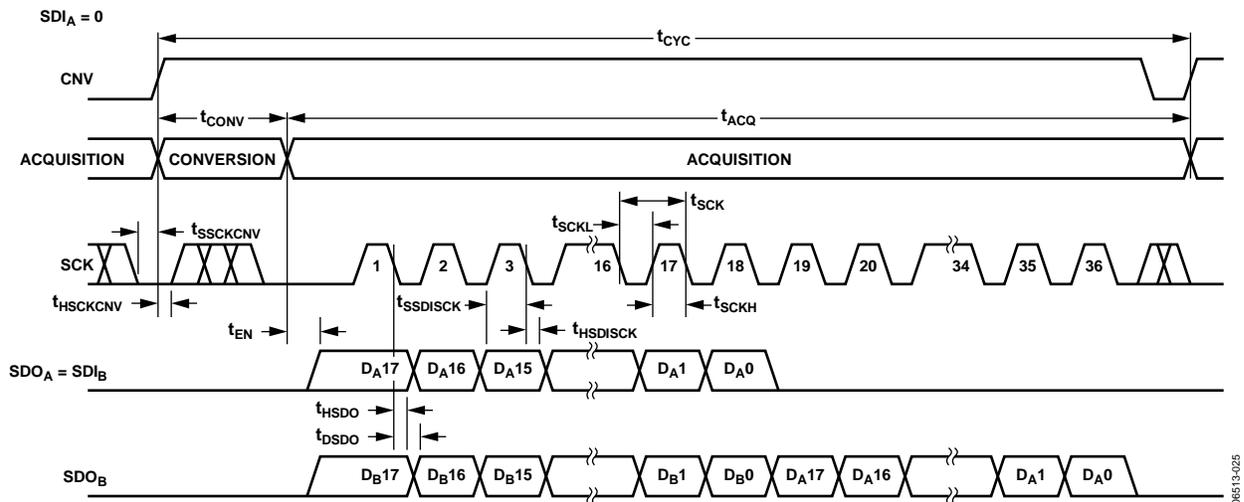


Figure 38. Chain Mode Without Busy Indicator Serial Interface Timing

CHAIN MODE WITH BUSY INDICATOR

This mode can also be used to daisy-chain multiple AD7982s on a 3-wire serial interface while providing a busy indicator. This feature is useful for reducing component count and wiring connections, for example, in isolated multiconverter applications or for systems with a limited interfacing capacity. Data readback is analogous to clocking a shift register.

A connection diagram example using three AD7982s is shown in Figure 39, and the corresponding timing is given in Figure 40.

When SDI and CNV are low, SDO is driven low. With SCK high, a rising edge on CNV initiates a conversion, selects the chain mode, and enables the busy indicator feature. In this mode, CNV is held high during the conversion phase and the

subsequent data readback. When all ADCs in the chain have completed their conversions, the SDO pin of the ADC closest to the digital host (see the AD7982 ADC labeled C in Figure 39) is driven high. This transition on SDO can be used as a busy indicator to trigger the data readback controlled by the digital host. The AD7982 then enters the acquisition phase and powers down. The data bits stored in the internal shift register are clocked out, MSB first, by subsequent SCK falling edges. For each ADC, SDI feeds the input of the internal shift register and is clocked by the SCK falling edge. Each ADC in the chain outputs its data MSB first, and $18 \times N + 1$ clocks are required to read back the N ADCs. Although the rising edge can be used to capture the data, a digital host using the SCK falling edge allows a faster reading rate and consequently more AD7982s in the chain, provided the digital host has an acceptable hold time.

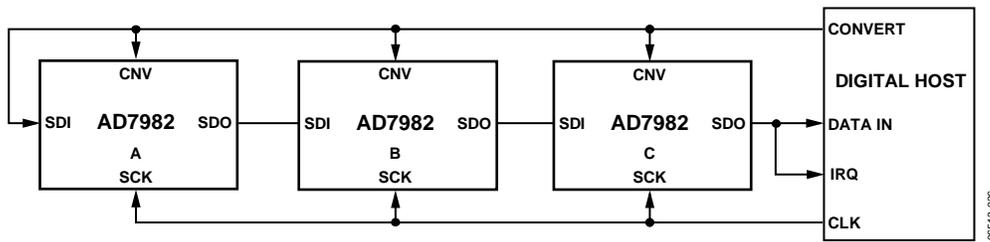


Figure 39. Chain Mode with Busy Indicator Connection Diagram

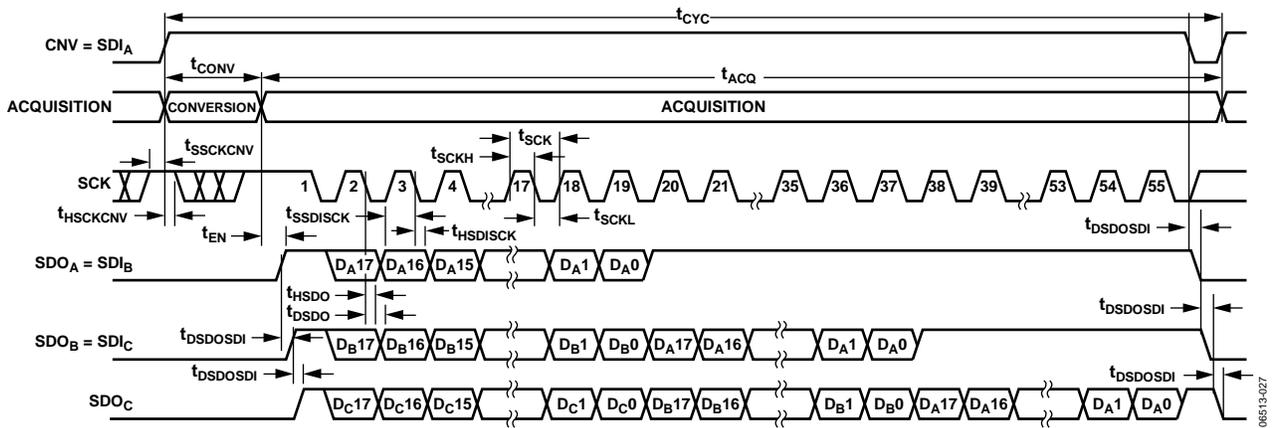


Figure 40. Chain Mode with Busy Indicator Serial Interface Timing

APPLICATION HINTS

LAYOUT

The printed circuit board that houses the AD7982 should be designed so that the analog and digital sections are separated and confined to certain areas of the board. The pinout of the AD7982, with its analog signals on the left side and its digital signals on the right side, eases this task.

Avoid running digital lines under the device because these couple noise onto the die, unless a ground plane under the AD7982 is used as a shield. Fast switching signals, such as CNV or clocks, should not run near analog signal paths. Crossover of digital and analog signals should be avoided.

At least one ground plane should be used. It can be common or split between the digital and analog sections. In the latter case, the planes should be joined underneath the AD7982s.

The AD7982 voltage reference input REF has a dynamic input impedance and should be decoupled with minimal parasitic inductances. This is done by placing the reference decoupling ceramic capacitor close to, ideally right up against, the REF and GND pins and connecting them with wide, low impedance traces.

Finally, the power supplies VDD and VIO of the AD7982 should be decoupled with ceramic capacitors, typically 100 nF, placed close to the AD7982 and connected using short, wide traces to provide low impedance paths and to reduce the effect of glitches on the power supply lines.

An example of layout following these rules is shown in Figure 41 and Figure 42.

EVALUATING AD7982 PERFORMANCE

Other recommended layouts for the AD7982 are outlined in the documentation of the evaluation board for the AD7982 ([EVAL-AD7982SDZ](#)). The evaluation board package includes a fully assembled and tested evaluation board, documentation, and software for controlling the board from a PC via the [EVAL-SDP-CB1Z](#).

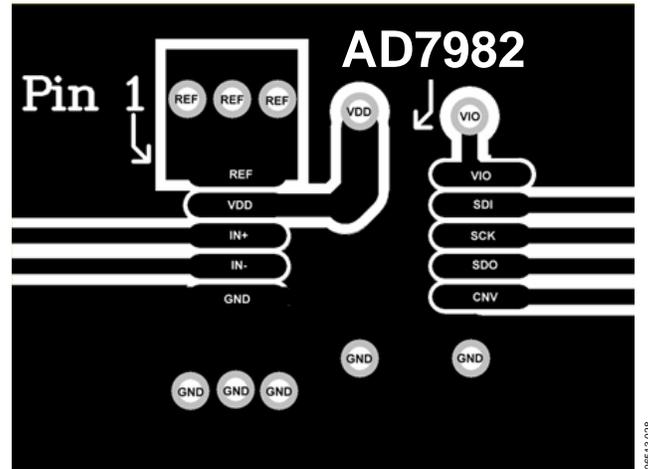


Figure 41. Example Layout of the AD7982 (Top Layer)

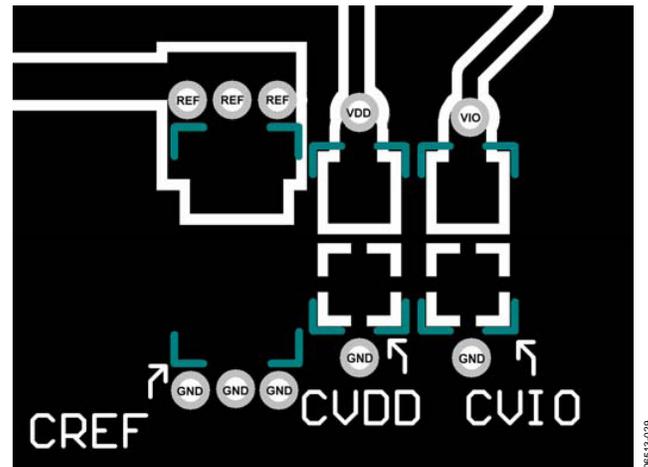
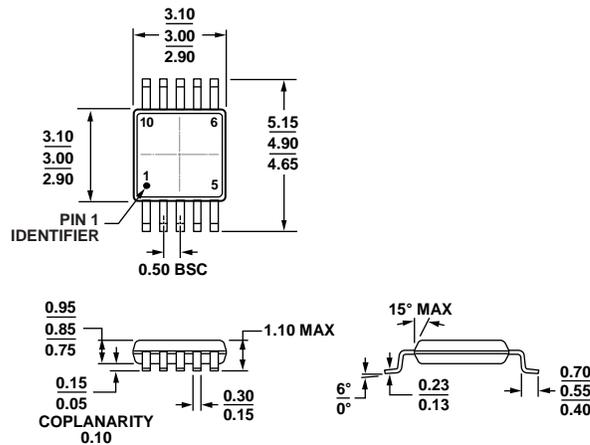


Figure 42. Example Layout of the AD7982 (Bottom Layer)

OUTLINE DIMENSIONS



COMPLIANT TO JEDEC STANDARDS MO-187-BA

Figure 43. 10-Lead Mini Small Outline Package [MSOP] (RM-10)

Dimensions shown in millimeters

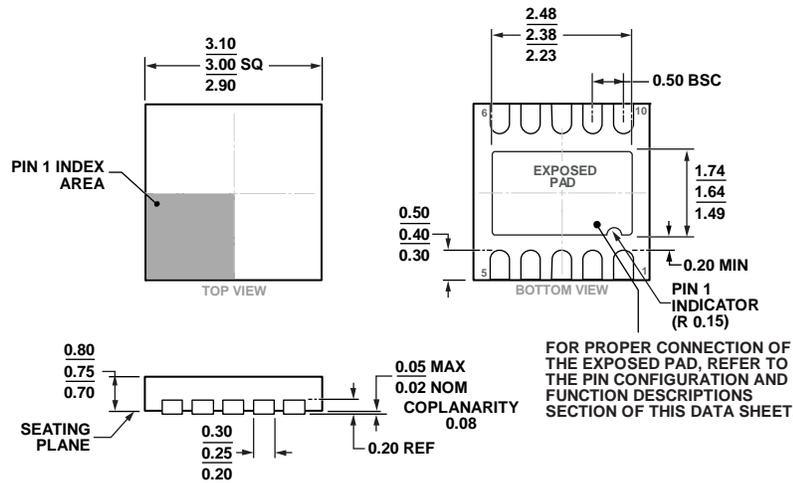


Figure 44. 10-Lead Lead Frame Chip Scale Package [QFN (LFCSP_WD)]

3 mm x 3 mm Body, Very Very Thin, Dual Lead

(CP-10-9)

Dimensions shown in millimeters

ORDERING GUIDE

Model ¹	Notes	Temperature Range	Package Description	Package Option	Ordering Quantity	Branding
AD7982BRMZ		-40°C to +85°C	10-Lead MSOP	RM-10	Tube, 50	C5F
AD7982BRMZRL7		-40°C to +85°C	10-Lead MSOP	RM-10	Reel, 1000	C5F
AD7982BCPZ-RL7		-40°C to +85°C	10-Lead QFN (LFCSP_WD)	CP-10-9	Reel, 1500	C5F
AD7982BCPZ-RL		-40°C to +85°C	10-Lead QFN (LFCSP_WD)	CP-10-9	Reel, 5000	C5F
EVAL-AD7982SDZ	²		Evaluation Board			
EVAL-SDP-CB1Z	³		Controller Board			

¹ Z = RoHS compliant part.

² This board can be used as a standalone evaluation board or in conjunction with the EVAL-SDP-CB1Z for evaluation/demonstration purposes.

³ This board allows a PC to control and communicate with all Analog Devices evaluation boards ending in the SDZ designator.